

Observer-based Transient Frequency Drift Compensation in AC Microgrids

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Abstract—This paper proposes a novel solution for transient frequency compensation in weak 3-phase Microgrids (MGs) based on a Luenberger observer and a transient frequency detector. Unlike in conventional grids, the low inertia of the generators coupled to a MG could make their rotor speeds to be affected by load changes, varying the grid frequency and compromising the grid quality and stability. This problem has been approached in the literature by the Virtual Inertia (VI) concept. However, the existing solutions are affected by the decoupling of the grid frequency reference and the frequency estimation bandwidth. The proposed paper addresses these problems by the use of a transient frequency drift estimator based on a transient detector and a Luenberger type observer that provides a nearly-zero lag frequency estimation. The proposed alternative is analytically compared with the existing techniques and validated through simulation and exhaustive experimental results in an islanded MG. The developed method enables a 1Hz reduction in the transient frequency deviation when compared with the existing alternatives and improves the system stability.

Index Terms—AC-DC, DC-DC power converters, Energy storage, Frequency control, Microgrids, Observers, Power control, Power quality, Power system dynamics.

I. INTRODUCTION

THE weakness, quality and stability problems associated to Microgrids (MGs) have been considered since they emerged, demanding a significant research effort [1]–[3]. Distribution Static Synchronous Compensator (D-STATCOM) with Energy Storage, or simply Energy Storage System (ESS), are the preferred solution for power quality enhancement involving active power exchange in MGs [4]–[6].

Some examples of ESS use can be found for frequency profile enhancement [7], [8]. In these applications, the ESS works in coordination with a power plant, using a communication link and providing access to the system variables. Often, the ESS participates both in the power sharing during steady state and transients. In [3], an ESS system was proposed for frequency compensation limited to the operation during transients. However, the proposed solution relies on the commu-

nication with the generation system. The communication-less frequency compensation in MGs has been already proposed, being one of the most common solutions the Virtual Inertia (VI) [9]–[16].

The absence of communications leads to three main constraints: 1) The grid frequency must be estimated from the voltage signals at the point of common coupling (PCC). Methods such as Phase-Locked Loop (PLL) [17], [18], or more robust techniques as Frequency-Locked Loop (FLL) [19], can be used. However, they are characterized by relatively slow dynamics which limits the compensator controller bandwidth. 2) Improved load-disturbance rejection capability needs for a derivative action to fasten the controller response, however this is prone to noise in the estimated frequency signal. 3) Avoiding power sharing during steady state might be compromised with varying grid frequency reference.

The present paper will focus on the design of an improved transient frequency drift compensator (TFDC) for its application in weak MGs. The TFDC will be implemented by means of a D-STATCOM with ESS, being the proposed method agnostic with respect to the ESS technology. Although other enhanced solutions appear in the literature [20]–[24], in the present study, two of the main existing limitations for frequency compensation are addressed: the decoupling of the grid frequency reference and the low bandwidth of grid frequency estimators. The performance achieved by existing feedback control has been improved by the development of a transient observer, formed by a novel transient detection method based on signal correlation that effectively decouples the grid reference frequency from the compensator inputs, and a Luenberger-based observer that provides a nearly-zero lag frequency estimation and allows to increase the phase margin in the frequency controller. Among the contributions in the present paper, it is worth to highlight: 1) an exhaustive system characterization and disturbance rejection analysis of the existing methods compared with the proposed TFDC, 2) a novel method for the detection of the transient frequency and 3) the implementation of a novel enhanced solution based on the use of a Luenberger type observer [25] for the grid frequency estimation that allows for a reduction of the compensator phase lag, mitigating the dependence on the derivative factor associated to VI.

The proposed techniques have been compared with the existing ones, analytically and experimentally, in an isolated MG with resistive and Constant Power Loads (CPL), evincing the limitations of VI and existing frequency estimators when used for transient frequency compensation. A normalized

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The generator mechanical system is coupled to its electrical counterpart, thus any change or disturbance in the electrical grid will be reflected in its mechanical system. When an electrical load demanding active power is suddenly connected to the grid, it will generate an equivalent load torque proportional to the load current at the generator's shaft. This torque will be seen as a disturbance by the governor, causing a speed variation which depends on the mechanical inertia and the governor control system. Considering the control system of the governor as a PI regulator in the ideal form $C_g(s) = K_p \cdot (1 + \frac{1}{sT_i})$, and neglecting the dynamic contribution of the generator electrical subsystem, the disturbance transfer function D_g is given by (1).

$$D_g(s) = \frac{-\omega_r(s)}{T_L(s)} = \frac{G_{gen}(s)}{1 + C_g(s)G_{gen}(s)} = \frac{\frac{1}{J}s}{s^2 + \frac{K_p+b}{J}s + \frac{K_p}{T_i J}} \quad (1)$$

For future use and analysis in this paper, $D_g(s)$ is reformulated by a general 2nd order expression (2).

$$D_g(s) = \frac{k_g \omega_{ng}^2 s}{s^2 + 2\xi_g \omega_{ng} s + \omega_{ng}^2} \quad (2)$$

If the governor is considered as an ideal PI regulator, the parameters are equivalent to $k_g = \frac{T_i}{K_p}$, $\omega_{ng} = \sqrt{\frac{K_p}{T_i J}}$ and $\xi_{ng} = \frac{b+K_p}{2J\omega_{ng}}$.

It is worth noting that not only the frequency but also the generator voltage is proportional to the mechanical speed through the back electromotive force constant. Therefore, the compensation could positively affect both the active and reactive power sharing.

III. TRANSIENT FREQUENCY DRIFT COMPENSATION

The basic idea of the dynamic frequency drift compensation consists in maintaining the active power balance between the grid elements during transients. In the case under study, the transient active power mismatch between the generation and consumption in the grid will depend on the grid equivalent inertia determined by the synchronous generators. For that reason, one of the first ideas that emerged consisted in introducing a VI by using an ESS that emulates the behavior of a synchronous generator, known in the literature as Virtual Synchronous Machine (VSM) [20]. The controller is defined by the pseudo-derivative feedback regulator (PDF), [27], given by (3).

$$T_{ESS}(t) = k_{pESS}(w_e^*(t) - w_e(t)) - J_{ESS} \cdot \frac{d}{dt} w_e(t) \quad (3)$$

Where T_{ESS} is the equivalent torque, k_{pESS} the damping coefficient, J_{ESS} the virtual inertia gain, w_e the instantaneous grid frequency and w_e^* the grid frequency reference. The conditions and constraints of the proposed communication-less solution are the following:

- There is not communication between the proposed solution and any other system at the grid.
- Only the currents and voltages at the PCC are available.
- The control relies on the the estimated grid frequency.

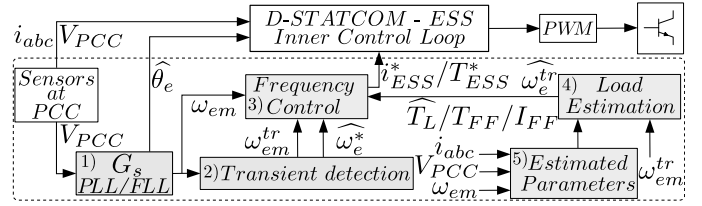


Fig. 3. Simplified control scheme for the proposed system.

- The paper is focused on improving the transient frequency drift, limiting the power exchange between the proposed system and the grid.
- The grid frequency command in the MG (w_e^*) is unknown.
- The possibility of binding the proposed solution to a significant load in the grid, gaining access to the load current, is also considered.

Under these constraints, the main problems to be tackled are summarized as:

- The frequency has to be estimated from electrical variables. The effects of measurement noise and delays as well as grid distortion over the used frequency estimation techniques must be considered.
- The transient state has to be detected in order to avoid active power injection during the steady-state. The steady-state frequency command must be decoupled.
- The use of derivative terms may compromise the reliability under noisy conditions.

A. Proposed Control System

The proposed control system scheme is shown in Fig. 3. Besides the internal current control loops, five blocks can be identified forming the compensator control.

1) *Grid synchronization and frequency estimation*: It provides the estimated grid angle ($\hat{\theta}_e$) and the estimated grid frequency (ω_{em}). It is based on PLL, DSOGI-FLL techniques [17]–[19] or any other frequency estimation method. The transient performance has been experimentally evaluated in Fig. 4, using the generator speed measurement given by a resolver as a reference for red the comparison. Both PLL with low pass filter and FLL are good candidates for the frequency estimation. Due to its robustness under distorted grids, a DSOGI-FLL will be used in this paper. Its dynamic transfer function will be referred henceforth as $G_s(s)$, modeled as the 2nd order system approximation in (4), obtained by curve-fitting methods.

$$G_s(s) = \frac{\omega_{em}}{\omega_e} = \frac{k_s \omega_{ns}^2}{s^2 + 2\xi_s \omega_{ns} s + \omega_{ns}^2} \quad (4)$$

Where k_s is the sensor gain, 1 by default, and ω_{ns} , ξ_s are the natural frequency and damping factor of the system respectively.

2) *Transient detection*: To avoid steady-state compensation, the detection of the frequency transients is required and the actual grid frequency command has to be decoupled. The proposed method is detailed at section III-B.

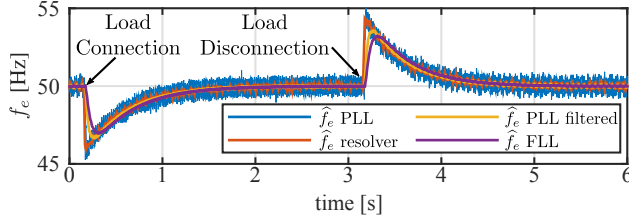


Fig. 4. Experimental results for the frequency drift measurement at the PCC under the connection and disconnection of a resistive load without compensation. The used setup is defined by Fig. 1 and Table II.

3) *Frequency control*: The main block of the control system consist in a feedback regulator able to provide a current or torque reference for the D-STATCOM (i_{ESS}^* , T_{ESS}^*), using the error between the frequency reference and the frequency estimation. Details for the feedback based control are given at section III-C.

4) *Load disturbance estimation*: When grid parameters are known or estimated, it is possible to generate a load estimation and use it as a feed-forward, either in terms of power, torque or current (T_{FF} , I_{FF}) to improve the dynamic response [8]. In this study, two options have been considered. One is based on the current measurement, developed at section III-D, and another relying on a Luenberger-based observer, considered at section IV.

5) *Estimated parameters*: The necessary information for the implementation of the load disturbance observer should be estimated either on-line or off-line. In the scope of this paper all the parameters will be known or obtained off-line.

B. Transient detection

The transient detection issue has been already covered in previous literature by 1) using a transient detection window [3], and 2) an open loop estimator to extract the frequency reference considering a droop-controlled grid [28]. In the first case, a simple comparison of the feedback frequency and a threshold determines a transient window. However, delays, noise and harmonic distortion in the frequency estimator may lead to incorrect performance. In the second case, the open loop estimator leads to errors with any change in the estimator parameters. In this paper, a method based on the correlation of the measured frequency with a signal of period T and zero average is proposed (5).

$$C\omega_e(t) = \int_0^T x(t)f(t)dt \rightarrow C^2\omega_e(t) = \left(\int_0^T x(t)f(t)dt \right)^2 \quad (5)$$

where $C\omega_e$ is the correlation result, $x(t)$ is ω_{em} and $f(t)$ could be any function having zero average. For the sake of simplicity, a sine type function is used.

Assuming that the grid frequency reference will have a slow variation compared to the integration interval, T , the correlation function will give low values during the steady state. On the other hand, when a transient frequency drift occurs, it will lead to larger values. The resulting behavior is similar to the use of a derivative, but without the associated

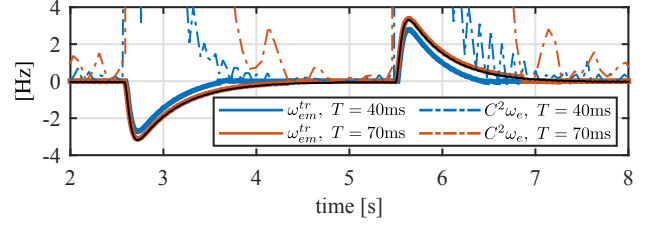


Fig. 5. Experimental results for the transient frequency estimation using the proposed method. Evaluation under connection and disconnection of a resistive load at the PCC without compensation. The setup is defined by Fig. 1 and Table II.

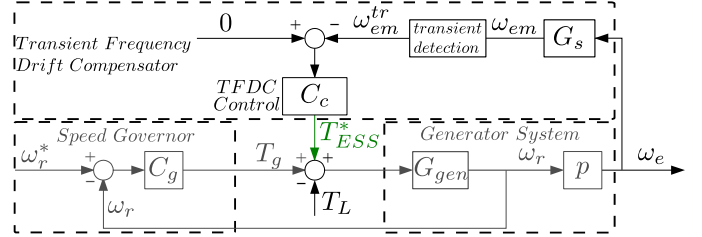


Fig. 6. Proposed controller for transient frequency drift compensation in the grid model block diagram. The speed governor and generator blocks match the system presented in Fig. 2. The torque provided by the TFDC is highlighted in green.

noise problems. Using the correlation squared value, (5), a transient window is generated and any frequency out of that window is considered to be the the grid frequency reference (ω_e^*). The last frequency value before the transient detection is considered as the estimated reference frequency ($\widehat{\omega_e^*}$). The transient detector output is the transient frequency ($\widehat{\omega_{em}^{tr}}$), obtained as $\omega_{em}^{tr} = \omega_{em} - \widehat{\omega_e^*}$.

The obtained experimental results for the estimated transient frequency are shown at Fig. 5. Two different T values are used for the estimation: $T = 40\text{ms}$ and $T = 70\text{ms}$. The correlation value is scaled by 10 to simplify the representation. Threshold value is set to 5 and the FLL bandwidth is set to 5Hz. The results are compared with respect to the measured frequency, from which the reference value has been subtracted.

C. Frequency feedback based control

The feedback based frequency control is shown in Fig. 6. The TFDC controller C_c , uses the estimated transient frequency (ω_{em}^{tr}), obtained from the frequency sensor and the transient detection block, to provide a control action by means of an equivalent torque command (T_{ESS}^*).

Once the TFDC is included in the system, the disturbance rejection transfer function $\frac{\omega_r}{T_L}$ is given by (6)

$$D_c(s) = \frac{\omega_r(s)}{T_L(s)} = -\frac{D_g(s)}{1 + D_g(s) \cdot C_c(s) \cdot G_s'(s)} \quad (6)$$

where $G_s'(s) = G_s(s) \cdot p$, p is the number of pole pairs of the machine and $G_s(s)$ the sensor transfer function. $D_g(s)$ is the generator disturbance transfer function in (2). The obtained expression only applies during the transient, assuming the grid frequency reference has been already decoupled.

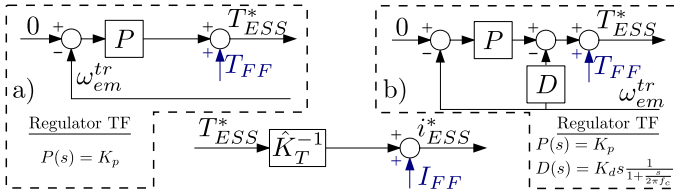


Fig. 7. Control structure for frequency drift compensation. a) Proportional (P) regulator; b) Pseudo-derivative feedback (PDF) structure. An optional load feed-forward can be applied either in terms of torque, T_{FF} , or current, I_{FF} .

Fig. 7 shows the general scheme for the frequency controller C_c , including the torque to current conversion. A feed-forward to improve the control is considered as an optional functionality (T_{FF} , I_{FF}).

It is worth noting that PI regulators are not considered in this study as the use of an integral action in the controller, even if it can improve the steady state disturbance rejection drastically, would also lead to the unavoidable share of power during steady state. P and PDF options will be analyzed. The two alternative transfer functions of the feedback frequency controller $C_c(s)$ are defined by (7), P, and (8), PDF regulator, assuming the input as $-\omega_{em}^{tr}$.

$$C_c(s) = K_p \quad (7) \quad C_c(s) = K_p + K_d s \frac{2\pi f_c}{2\pi f_c + s} \quad (8)$$

Where K_p and K_d are the proportional and derivative gains of the compensator. These two gains are equivalent to the damping coefficient k_{pESS} and the virtual inertia gain J_{ESS} in (3) respectively. The variable f_c is the cut-off frequency of the low-pass filter associated to the derivative term.

The different alternatives are compared based on their dynamic stiffness, defined as (9).

$$S_c(s) = \frac{T_L(s)}{\omega_r(s)} = \frac{1 + D_g(s) \cdot C_c(s) \cdot G'_s(s)}{D_g(s)} \quad (9)$$

Fig. 8 shows the dynamic stiffness evaluated in frequency domain and the corresponding transient response in time domain for two different P and PDF settings. Two different proportional gains providing two different gain margins (GM) are used. In the case of the PDF, a minimum phase margin of 60° is set at the open-loop crossover frequency in both cases. The graph shows the benefits of an increased proportional gain and the improved disturbance rejection capability provided by the inclusion of the differential term. As shown in time domain, the predicted benefits for including the differential term are translated to a reduced initial overshoot when compared to the P method.

Finally, the experimental results for the feedback-based compensation are shown in Fig. 9. A good agreement with respect to the previous theoretical discussion can be observed.

D. Load feed-forward and state observation

Enhanced dynamic response for the transient frequency drift controller can be obtained by the use of feed-forward disturbance decoupling and the increase of the frequency estimation bandwidth by using a Luenberger type observer.

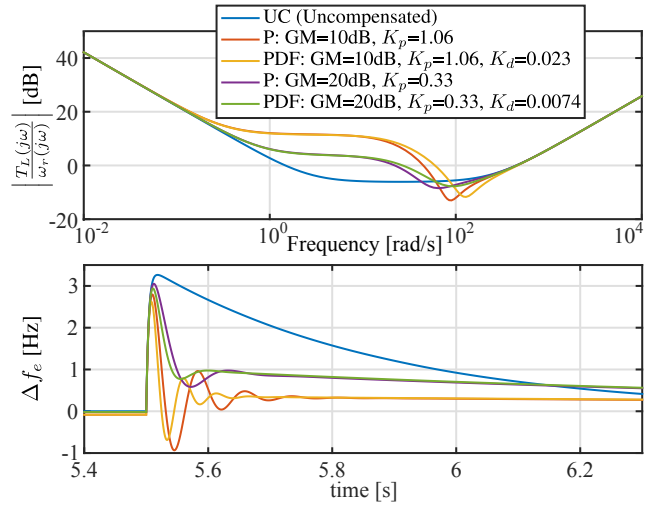


Fig. 8. Performance comparison of the P and PDF methods. Top: dynamic stiffness. Bottom: transient response.

If the load demand is available, it can be used as a feed-forward for the controller, as shown in Fig. 7. Ideally, if the load is fully known, the frequency drift will be eliminated (grey line in Fig. 9). However, that solution would lead to the compensation of the whole load power also during steady state. In order to compensate only the transient and keep the grid frequency unalterable, the ESS has to provide the difference between the load power and the power drawn by the generator, i.e. the equivalent torque of the compensation system should be $T_{ESS} = T_L - T_g$. Nevertheless, in a communication-less system, the generator information is not available. However, the load information is still a valuable information as it is a derivative state of the frequency, allowing to anticipate the control reaction.

Fig. 9 shows the experimental performance comparison for the different feedback methods, considering different configurations, and the response when a load feed-forward is used. The shown signals correspond to the DSOGI-FLL frequency signal using a FLL BW = 25Hz. UC stands for the uncompensated case. P+FF and PDF+FF are the combination of P and PDF with a load feed-forward respectively. The feed-forward is filtered by a 2^{nd} order high-pass filter with bandwidth=0.5Hz. FC stands for the full load compensation obtained by equaling the D-STATCOM current reference to the load current. In this example, the load information comes from a load current sensor, which is a valid assumption if the proposed solution is to be coupled to a significant load.

IV. TRANSIENT FREQUENCY-DRIFT OBSERVER

The main purpose of the observer is to provide a transient frequency-drift estimation by providing a nearly zero phase-lag $\widehat{\omega}_e^{tr}$ estimation within the observer bandwidth. This will boost the response of the TFDC, being able to compensate frequency drift transients usually affected by the PLL/FLL bandwidth restrictions. Additionally, the proposed observer also provides an estimation of the load disturbance that could be used for the feed-forward compensation replacing the T_{FF} measurement

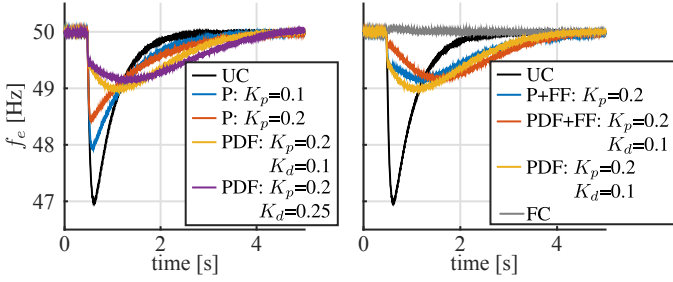


Fig. 9. Transient frequency drift compensation using different control methods under load connection transient. The setup is defined by Fig. 1 and Table II. Further details on the experimental setup are given at section V.

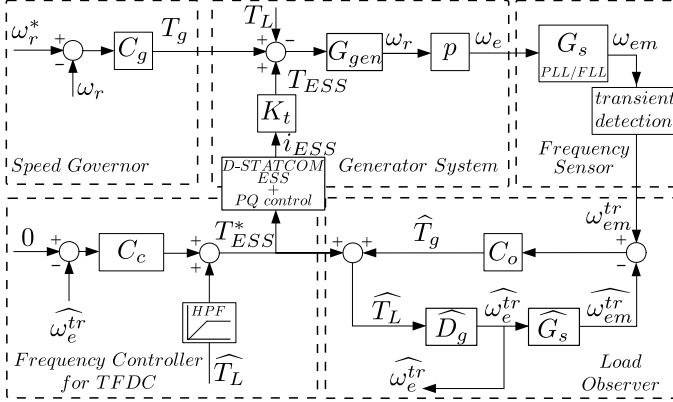


Fig. 10. Proposed observer control structure. The use of \widehat{T}_L is optional.

by the estimated load \widehat{T}_L . Although the paper proposes the use of such a load estimation, \widehat{T}_L , it is not used or validated in this study, being part of future development. The proposed Luenberger-based observer control is shown in Fig. 10, where C_o represents the transfer function of the observer regulator. It is worth to point out that in the case the observer is not used, ω_{em}^{tr} will be the feedback variable for the close loop frequency controller C_c .

As the generator and governor parameters are unknown, the C_g and G_{gen} transfer functions cannot be explicitly used in the proposed solution. However, the approximations proposed before for the sensor and the generator disturbance transfer functions (2), are appealing candidates for the observer implementation. The experimental comparison between the proposed approximations and the real systems are shown in Fig. 11. A really good matching is clearly observed. The observer is implemented using the state-space formulation corresponding to the model shown in Fig. 12. The model is defined by the state vector $x = [x_1, x_2, x_3, x_4]^T$, the input vector $u = [T_L]$ and the output vector $y = [\omega_e, \omega_{em}]^T = [p \cdot x_1, x_3]^T$. The state, input, output and feed-forward matrices are defined in (10).

$$A = \begin{bmatrix} -2\xi_g\omega_{ng} & -\omega_{ng}^2 & 0 & 0 \\ 1 & 0 & 0 & 0 \\ 0 & 0 & 0 & 1 \\ k_s p \omega_{ns}^2 & 0 & -\omega_{ns}^2 & -2\xi_s\omega_{ns} \end{bmatrix}, B = \begin{bmatrix} k_g \omega_{ng}^2 \\ 0 \\ 0 \\ 0 \end{bmatrix}$$

$$C = \begin{bmatrix} p & 0 & 0 & 0 \\ 0 & 0 & 1 & 0 \end{bmatrix}, D = \begin{bmatrix} 0 \end{bmatrix} \quad (10)$$

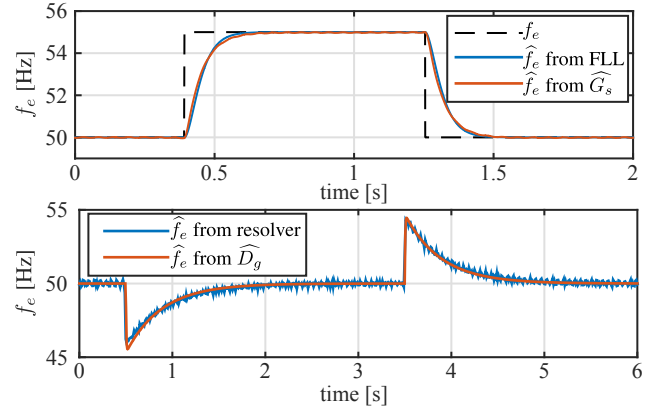


Fig. 11. Experimental results. Top: DSOGI-FLL response and its approximation using the 2nd order transfer function \widehat{G}_s . Bottom: Open-loop response obtained with the estimation of the disturbance transfer function \widehat{D}_g compared with the frequency measured by the generator resolver.

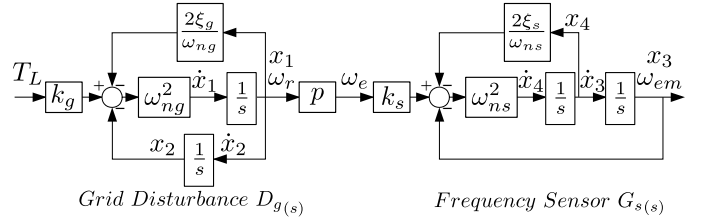


Fig. 12. Observer block diagram in state space form.

The dynamic stiffness for the proposed observer block diagram, assuming parameters matching between the real and the observed systems, is defined by (11).

$$\frac{T_L(s)}{\omega_e(s)} = \frac{1 + \widehat{D}_g(s) \cdot C_o \cdot \widehat{G}_s(s)}{1 + \widehat{D}_g(s)(C_c(s) + C_o(s) \cdot \widehat{G}_s(s))} \quad (11)$$

The observer controller, $C_o(s)$, consists in a 4th order transfer function, presenting the same order as the observed plant. It has been tuned in frequency domain using loop-shaping, trying to maximize the bandwidth while giving enough stability margin. The selected values are listed in Table II. The resulting frequency and transient responses comparing the proposed observer technique and the FLL feedback technique are shown in Fig. 13 and Fig. 14. The uncompensated and ideal sensor cases are shown as a reference. Ideal sensor case is defined as frequency feedback control with $G_s(s) = 1$, i.e., there is not phase lag introduced by the frequency estimation. As it can be seen, the use of the observer noticeably improves the initial transient response due to the compensated sensor lag. Moreover, in Fig. 14, the transient response of the design system (left $\omega_{ns} = 31.4$ rad/s), is compared with the response when the bandwidth of frequency sensor is reduced by four (right $\omega_{ns} = 7.85$ rad/s), without changing the observer regulator parameters. The proposed observer-based method still presents a better response than the alternatives.

V. EXPERIMENTAL RESULTS

The proposed frequency-drift compensation have been experimentally evaluated. The experimental grid has been presented in Section II, Fig. 1, and the relevant parameters

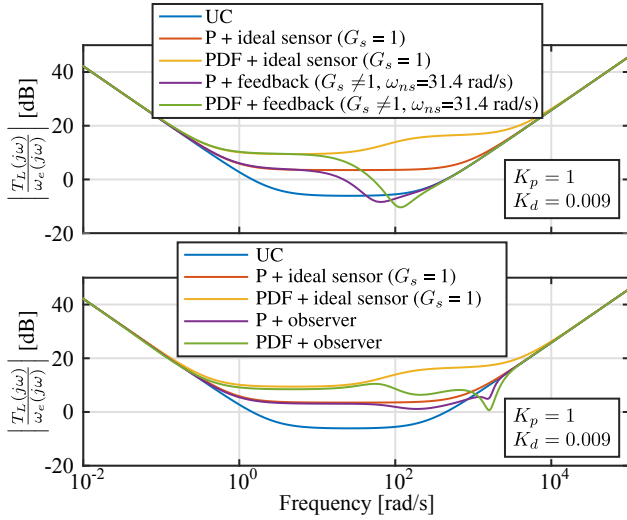


Fig. 13. Dynamic stiffness. Top: results for the feedback-based control. Bottom: observer-based control. The uncompensated and ideal sensor cases are shown as a reference.

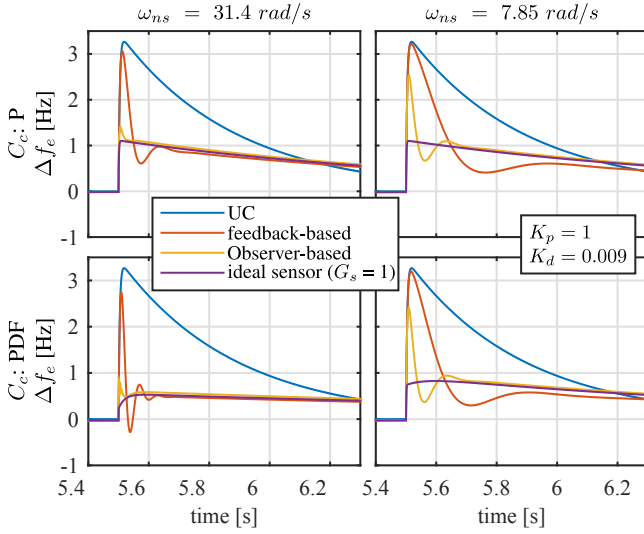


Fig. 14. Transient response comparison for different DSOGI-FLL bandwidth. Top: P controller. Bottom: PDF controller. Both cases are analyzed considering different feedback signals.

are given in Table II, including the P and PDF as well as the observer parameters used in the experimental tests. The equipment used to implement the experimental setup is shown in Fig. 15. The control system of the TFDC has been implemented in a TMS320F28335 DSC from Texas Instruments. The MG generator is emulated using 2 coupled PMSMs one acting as generator and other as the governor motor controlled by a commercial drive. The disturbances created by the different load types in the experimental MG, allow to test the effectiveness of the proposed observer-based compensator under a variety of conditions, enabling the comparison between the different existing methods which have been analyzed in this paper. It is worth noting that the grid frequency shown in the experimental results have been obtained using the speed resolver included in the industrial drive. The experimental results are obtained under two scenarios:

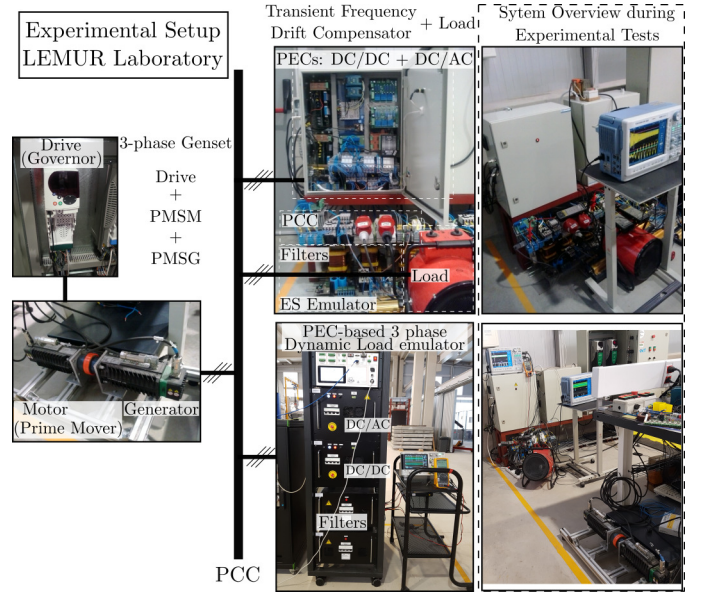


Fig. 15. Experimental prototype. Left: generator and drive used as the governor and the prime mover. Top center: TFDC and resistive load. Bottom center: dynamic load emulator based on PECs. Right: the setup during operation.

- 1) In the first scenario, the frequency variation for the evaluation of the TFDC is created by a load disturbance consisting in the connection and disconnection of a three-phase balanced resistive load. This test allows to be characterized and compare the different methods evaluating the response under a step disturbance, avoiding to have unwanted disturbances in the middle of a transient.
- 2) In the second scenario, a more realistic load behavior is pursued. In this case, the load disturbance is a CPL generated by the PECs-based dynamic load emulator. This second scenario allows to demonstrate the advantages of the proposed observer and its viability in a realistic MG environment, where the PECs operation might be compromised by the transient frequency and voltage magnitude drifts.

A comparison of the transient response for the feedback and feed-forward methods is shown in Fig. 16 for the first scenario. The load feed-forward is implemented using the measured load current, applying a 1st order high-pass filter with a cut-off frequency of 0.5Hz. The performance of the proposed observer-based solutions for the first scenario is shown in Fig. 17 compared with the feedback methods. As expected, feed-forward and the proposed observer-based methods have the best performance in terms of frequency compensation. Assuming that feed-forward methods need for extra sensors or/and communication, the proposed observer methods, that just depend on the voltage measurements at the PCC, are a promising alternative, offering an extra compensation at the beginning of the transient, reducing the maximum frequency deviation. In this particular case, for the selected parameters, the proposed methods P+Obs and PDF+Obs reduce the maximum frequency deviation in around 1Hz when compared with P and PDF methods without observer, i.e., using ω_{em}^{tr} instead

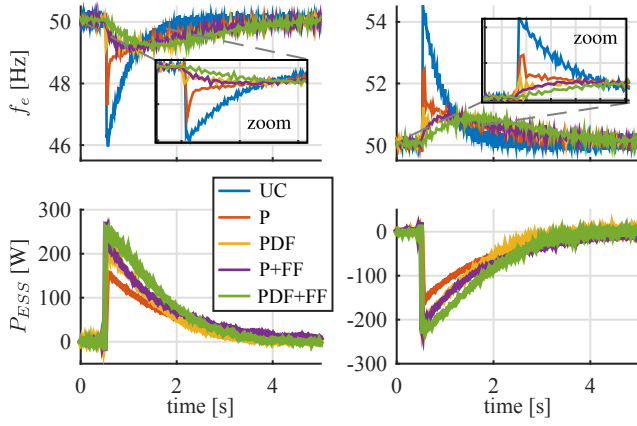


Fig. 16. Experimental results for the first scenario. Top: grid frequency obtained with the resolver. Bottom: power injected by the compensator. Left: load connection. Right: load disconnection.

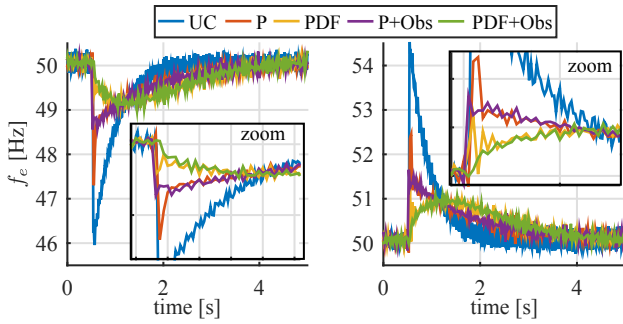


Fig. 17. Experimental results for the first scenario. Results using the proposed observer-based method. Grid frequency obtained with the resolver. Obs stands for observer-based compensation.

of $\hat{\omega}_e^{tr}$.

Although it has not been applied or tested in this paper, the observer provides an additional useful information. The observed load current, obtained from the estimation of \hat{T}_L , is represented in Fig. 18. As shown, the transient load disturbance can be estimated by a high-pass filter. This load estimation enables the implementation of a load feed-forward mechanism without the need for measuring the load current.

The results obtained for the second scenario using the PELs-based dynamic load emulator are shown in Fig. 19, for P and P+Obs methods, and in Fig. 21, for PDF and PDF+Obs. The frequency, the power drawn by the load emulator and the

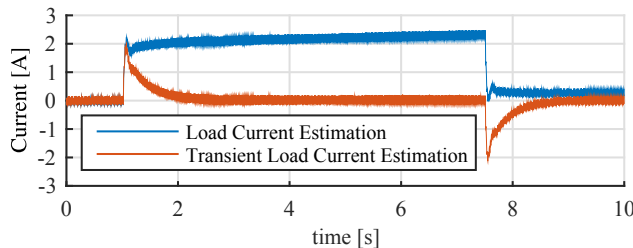


Fig. 18. Experimental results. Load current estimated by the observer. Full load current and transient load disturbance obtained by a 1st order high-pass filter with BW = 0.5Hz. The load current is 2.2A.

TABLE II
SYSTEM PARAMETERS

MG Voltage ph-ph / f_n	98V _{rms} / 50Hz
3-phase load	32 Ω
BEMF / Torque constant / Poles	98V/krpm / 1.6Nm / 3 pairs
Mechanical parameters	$J = 0.0019\text{kg} \cdot \text{m}^2$, $b = 0.2\text{Nms}$
Electrical parameters	$L_g = 6\text{mH}$, $R_g = 2.1\Omega$
Power / ESS Voltage	20kW / 140V
DC link voltage / Capacitor	300V / 2mF
Grid connected AC filter	$R = 0.2\Omega$, $L = 7.18\text{mH}$
DC/DC converter filter	$R = 0.1\Omega$, $L = 7.18\text{mH}$
TFDC DC/DC Current control	BW=500Hz, $K_{pi}=22$, $K_{ii}=13$
TFDC DC link Voltage control	BW=50Hz, $K_{pv}=1$, $K_{iv}=175$
TFDC AC/DC Current control	BW=400Hz, $K_{pi}=22$, $K_{ii}=50$
TFDC Control Gains	P : $K_p = 0.2$ PDF : $K_p = 0.2$, $K_d = 0.1$
Observer parameters	$k_g = 0.78$, $\omega_{ng} = 25.6$, $\xi_g = 4.96$ $k_s = 1$, $\omega_{ns} = 31.4$, $\xi_s = 1$
Observer C_o coefficients	$K_o = 10$, zeros=[10, 10, 5, 3.4] $\cdot 10^{-3}$ poles=[20, 10, 10, 6.67] $\cdot 10^{-4}$
Dynamic Load Emulator	Current BW = 500Hz Power BW = 50Hz Current limit = 10A Nominal Power = 1kW

power injected by the TFDC are represented. It is clearly seen the improvement in the the frequency profile with all methods when compared with the uncompensated case. In order to better compared them, Fig. 20 and 22 show the detailed view of the critical transients in the system.

The conclusions drawn from the experimental results can be summarized as: 1) for all the cases, the observer-based methods provide a reduction on the maximum frequency deviation when compared with the FLL feedback methods; 2) The maximum deviation is reduced by more than 1Hz in the case of P+Obs when compared with P and 3) when differential action is added, the proposed PDF+Obs method improves the frequency drift by more than 0.5Hz when compared with the PDF. All this conclusions demonstrate the viability and superiority of the proposed methods for fast frequency drift compensation.

Finally, a last test was performed in order to evaluate the limits of the different compensation methods under significant load steps. Fig. 23 shows the response of the system under 3 load steps, for five cases: uncompensated, P, P+Obs, PDF and PDF+Obs. The figure does not only show the effect of load disturbances in the frequency but also in the voltage magnitude, which is affected due to the generator impedance and the coupling between its speed and voltage. As shown in Fig. 23, at $t = 0.2\text{s}$, a load step of 600W is applied. Under this load condition, the load emulator trips for the uncompensated scenario due to an overcurrent as a result of the voltage magnitude and frequency distortion. At $t = 0.6\text{s}$, a load step of 750W is commanded. For this load value. the emulator trips for the P method, while it continues its operation for the rest of the methods. At $t = 1\text{s}$, when a 1kW load is applied, the emulator trips for the P+Obs and PDF methods, being still responsive when PDF+Obs is used for the compensation. This demonstrates the extended range of operation allowed by the proposed observer-based methods for transient frequency drift compensation.

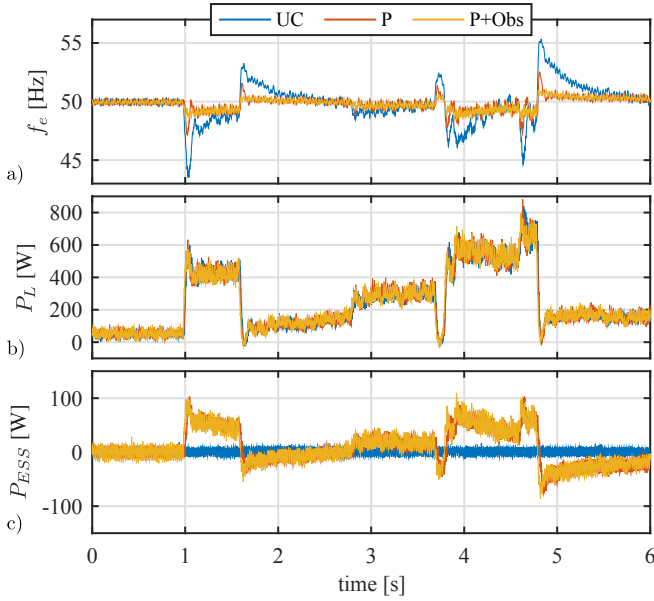


Fig. 19. Experimental results using the dynamic load emulator. a) grid frequency obtained with the drive resolver. b) load power consumption. c) active power injected by the compensator. P regulator and $P + Obs$ are compared.

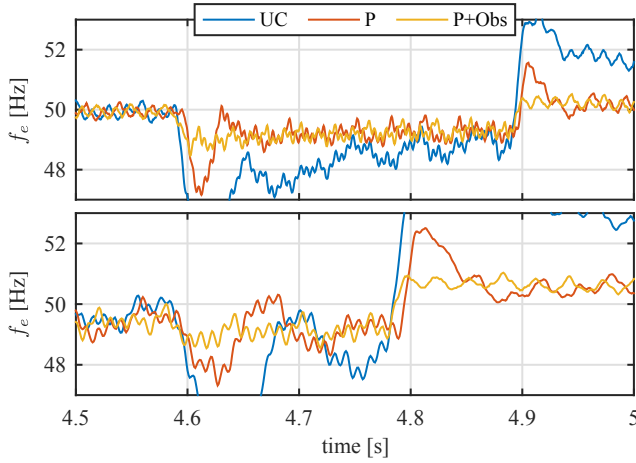


Fig. 20. Detailed view of the experiment in Fig. 19. Top: time zoom from $t = 0.5s$ to $t = 1.5s$. Bottom: time zoom from $t = 4.5s$ to $t = 5s$.

VI. CONCLUSION

In this paper, a transient frequency drift compensation has been proposed based on the use of a nearly-zero lag transient frequency estimation using a Luenberger observer. The proposed solution addresses two of the main limitations of existing frequency compensation methods in the literature: the phase lag on the frequency estimation, and the transient detection for decoupling the grid reference frequency. The performance achieved by feedback control has been improved by the development of a transient observer, formed by a novel transient detection method, based on signal correlation that effectively decouples the grid reference frequency from the compensator inputs, and a Luenberger-based observer that provides a fast frequency estimation and allows to increase the phase margin in the frequency controller. Moreover, the de-

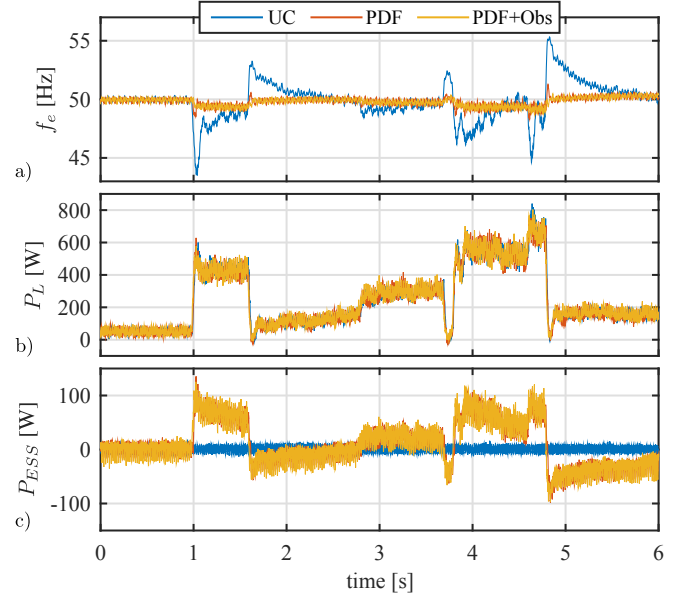


Fig. 21. Experimental results using the dynamic load emulator. a) grid frequency obtained with the drive resolver. b) load power consumption. c) active power injected by the compensator. PDF regulator and $PDF + Obs$ are compared.

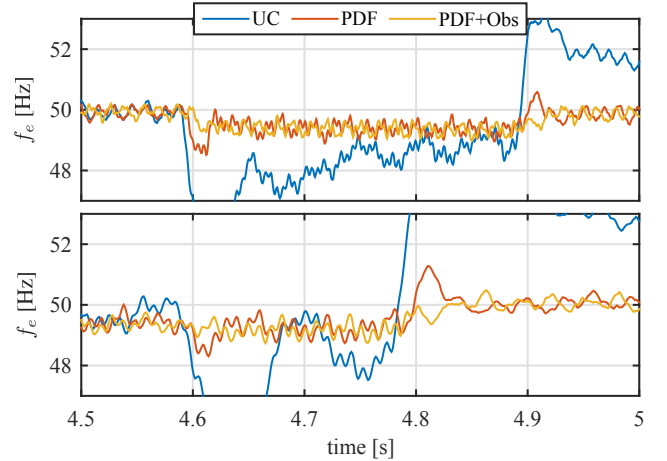


Fig. 22. Detailed view of the experiment in Fig. 21. Top: time zoom from $t = 0.5s$ to $t = 1.5s$. Bottom: time zoom from $t = 4.5s$ to $t = 5s$.

veloped observer structure allows to estimate the load torque, that can be employed as a feed-forward mechanism for the decoupling of the load disturbance. A detailed comparison, including analytical derivations, simulation and experimental results, have been carried out. The methods have been tested under two different scenarios considering passive and active loads based on resistors and PEC respectively. The analytical derivations, the simulation and the experimental results have demonstrated the effectiveness of the proposed observer-based TFDC. Additionally, it has been demonstrated that the proposed method allows for an extended range operation, withstanding higher disturbances and improving the system stability. The decoupling of the grid frequency reference makes the method suitable for the operation in weak grids under droop control. Finally, a comparative evaluation of

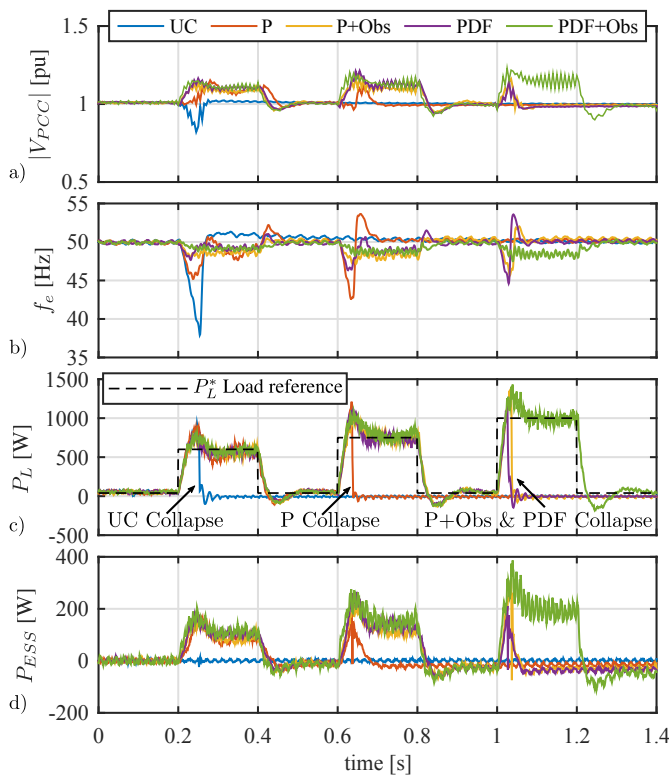


Fig. 23. Evaluation of the compensation methods under different load step disturbances introduced by the dynamic load emulator. a) Voltage magnitude at the PCC. b) Grid frequency obtained with the drive resolver. c) Load power consumption. d) Active power injected by the compensator.

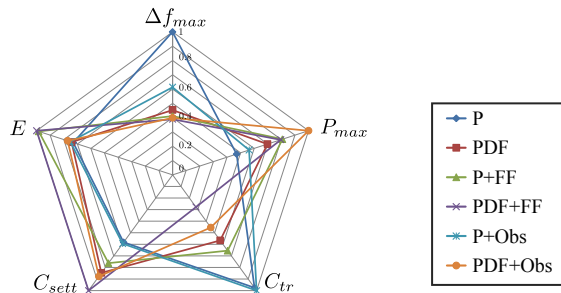


Fig. 24. Merit figure. Performance evaluation for all the considered methods. Δf_{max} : maximum frequency deviation, P_{max} : peak power E : total shared energy, C_{tr} : initial transient deviation, C_{sett} : settling time for transient frequency drift.

the analyzed techniques has been done, summarizing their performance in Fig. 24. Five indexes are considered. The indexes have been derived from the data obtained in the first scenario using a resistive load and are normalized in p.u., being all of them the higher the worst.

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